

Research Article

Optimal Vibration Control for Half-Car Suspension on In-Vehicle Networks in Delta Domain

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The paper explores the optimal vibration control design problem for a half-car suspension working on in-vehicle networks in delta domain. First, the original suspension system with ECU-actuator delay and sensor-ECU delay is modeled. By using delta operators, the original system is transformed into an associated sampled-data system with time delays in delta domain. After model transformation, the sampled-data system equation is reduced to one without actuator delays and convenient to calculate the states with nonintegral time delay. Therefore, the sampled-data optimal vibration control law can be easily obtained deriving from a Riccati equation and a Stein equation of delta domain. The feedforward control term and the control memory terms designed in the control law ensure the compensation for the effects produced by disturbance and actuator delay, respectively. Moreover, an observer is constructed to implement the physical realizability of the feedforward term and solve the immeasurability problem of some state variables. A half-car suspension model with delays is applied to simulate the responses through the designed controller. Simulation results illustrate the effectiveness of the proposed controller and the simplicity of the designing approach.

1. Introduction

In the past years, communication networks have been applied greatly and widely into the advanced vehicle systems, such as electronic control units (ECUs), sensors, and actuators which are all connected over the high-speed in-vehicle networks (IVNs), for example, Local Interconnect Network, Controller Area Network, Media Oriented Systems Transport [1–3], and so forth. However, in this kind of IVNs, two important issues emerge for the controller design problems. One is the network-induced delay issue. Over communication networks, the time delays generated between sensor-controller, controller-actuator, ECU computation delay, and so forth are unavoidably encountered. As well known, even a small time delay can make the systems disastrously unstable or generate oscillations [4–6]. So, this issue should be taken into account when we design a controller for a system over networks. The next issue is the system modeling problem. Actually, signals processed by microprocessors are digital,

and most of those produced by sensors or put into actuators are analogs. Thus, the continuous-time plant is combined with a discrete-time controller, where A/D and D/A converts are used to combine these two different signals. Therefore, a sampled-data system is more appropriate for the reality of networked-control system. In previous studies, there are two main approaches to get the sampled-data systems, those are, indirect approach of continuous-time domain and direct approach of discrete-time domain. However, the former is only suitable for simple control algorithms, and the latter has two drawbacks: one is that the discrete-time model is unable to approach to its corresponding continuous-time one as the sampling frequency increases; and the other is that the discretized system can cause oscillations and unstable phenomenon as the sampling frequency increases.

Consequently, we present two strategies to deal with these above-mentioned issues. First, we introduce the delta operator approach to build a sampled-data model for the networked-control system due to its accurate approximation

to the continuous-time model under rapid sampling conditions [7–11]. This advantage can be demonstrated by citing an instance.

Consider a continuous-time system consisted of (A, B) in the state-space representation. The associated discrete-time system can be got as (A_z, B_z) with $A_z = e^{AT}$, $B_z = \int_0^T e^{At} dt B$, and T the sampling period. Alternatively, the associated sampled-data system in delta domain is (A_δ, B_δ) with $A_\delta = (A_z - I)/T$, $B_\delta = B_z/T$, and I a unit matrix. Apparently, $A_z \rightarrow I$, $B_z \rightarrow 0$ and $A_\delta \rightarrow A$, $B_\delta \rightarrow B$ while $T \rightarrow 0$.

From this instance, it is clear that the discrete-time model cannot approximate to its original continuous-time one when sampling fast. On the contrary, the delta-domain sampled-data one enables approximating to the continuous accurately. See that this is our reason to apply the delta operators approach modeling a sampled-data system for an IVNs-based suspension.

The other contribution of this paper is developing the model transformation method [11–13] to solve optimal vibration control (OVC) design problem for sampled-data systems with time delays in delta domain. The model transformation method is based on the finite spectrum assignment methodology [14], and we have developed it solving the OVC design problems for time-delay systems in continuous-time domain or in discrete-time domain. It was proved able to transform the original time-delay system into a delay-free one such that the original solution problem is reduced from an infinite-dimension space to a finite-dimension space, and so that the controller design problem is greatly simplified [11–14].

In brief, as a result, the obtained control law in this paper consists of a feedforward term and some control memory terms which can be stored in memories beforehand. Hence, the persistent road excitation suffered by suspension can be reduced via the feedforward term, and the time-delay effect of the system can be compensated by the control memory terms. At last, we carry out some simulations to validate the effectiveness and the simplicity of the designed OVC comparing with the open-loop system (OLS).

The paper's organization displays as follows. After this introduction of Section 1, in Section 2, the system description and problem formulation have been done. In Section 3, the OVC is designed accompanied with the observer-based control law design. Numerical examples are simulated in Section 4. Concluding remarks are given in Section 5.

2. Problem Statement

2.1. System Modeling. Consider a four-degree-of-freedom half-car model (referred to in [15]) where the suspension motion is determined by the following dynamic equations:

$$\begin{aligned} m_s \ddot{x}_c(t) + k_f [x_{sf}(t) - x_{uf}(t)] + k_r [x_{sr}(t) - x_{ur}(t)] \\ + b_f [\dot{x}_{sf}(t) - \dot{x}_{uf}(t)] + b_r [\dot{x}_{sr}(t) - \dot{x}_{ur}(t)] \\ = u_f(t - \tau) + u_r(t - \tau), \end{aligned}$$

$$\begin{aligned} I \ddot{\phi}(t) + l_f k_f [x_{sf}(t) - x_{uf}(t)] + l_r k_r [x_{sr}(t) - x_{ur}(t)] \\ + l_f b_f [\dot{x}_{sf}(t) - \dot{x}_{uf}(t)] + l_r b_r [\dot{x}_{sr}(t) - \dot{x}_{ur}(t)] \\ = l_f u_f(t - \tau) + l_r u_r(t - \tau), \\ - m_{uf} \ddot{x}_{uf}(t) + k_f [x_{sf}(t) - x_{uf}(t)] - k_{tf} [x_{uf}(t) - x_{rf}(t)] \\ + b_f [\dot{x}_{sf}(t) - \dot{x}_{uf}(t)] = u_f(t - \tau), \\ - m_{ur} \ddot{x}_{ur}(t) + k_r [x_{sr}(t) - x_{ur}(t)] - k_{tr} [x_{ur}(t) - x_{rr}(t)] \\ + b_r [\dot{x}_{sr}(t) - \dot{x}_{ur}(t)] = u_r(t - \tau), \end{aligned} \quad (1)$$

through Newton-Euler method. In this half-car suspension model, the sprung mass m_s and unsprung one m_u are separated by spring, damper, and actuator, which are placed in parallel. The tire of the vehicle is modeled as a spring. Vertical motion $x_c(t)$ and pitch motion $\phi(t)$ of the sprung mass are considered, as well as the vertical motion of the front unsprung mass $x_{uf}(t)$ and the rear one $x_{ur}(t)$.

Consider it working on an IVNs-based environment, as depicted in Figure 1, where x , u , and y_m denote the system state, control input, and measured output, respectively; v is the road excitation input; τ , σ are constant ECU-actuator delay and sensor-ECU delay, respectively, (actuator delay and sensor delay for short) which are always assumed to be known and constant in such IVNs environment.

With the purpose of replacing (1) into the state-space representation, define the state, control, and disturbance vectors as

$$\begin{aligned} x(t) &= [x_{sf}(t) - x_{uf}(t), x_{sr}(t) - x_{ur}(t), \\ & x_{uf}(t) - x_{rf}(t), x_{ur}(t) - x_{rr}(t), \\ & \dot{x}_{sf}(t), \dot{x}_{sr}(t), \dot{x}_{uf}(t), \dot{x}_{ur}(t)]^T, \\ u(t) &= [u_f(t), u_r(t)]^T, \\ v(t) &= [\dot{x}_{rf}(t), \dot{x}_{rr}(t)]^T, \end{aligned} \quad (2)$$

the controlled output vector as

$$\begin{aligned} y_c(t) &= [\ddot{x}_c(t), \ddot{\phi}(t), x_{sf}(t) - x_{uf}(t), x_{sr}(t) - x_{ur}(t), \\ & x_{uf}(t) - x_{rf}(t), x_{ur}(t) - x_{rr}(t)]^T \\ &= [\ddot{x}_c(t), \ddot{\phi}(t), x_1(t), x_2(t), x_3(t), x_4(t)]^T, \end{aligned} \quad (3)$$

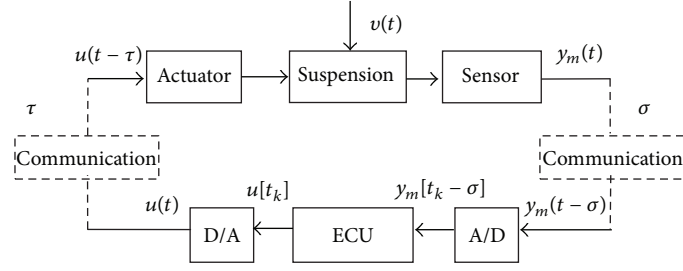


FIGURE 1: Suspension system working on IVNs.

and the measured output vector as

$$\begin{aligned} y_m(t) &= [x_{sf}(t - \sigma) - x_{uf}(t - \sigma), \\ &\quad x_{sr}(t - \sigma) - x_{ur}(t - \sigma), \dot{x}_{sf}(t - \sigma), \dot{x}_{sr}(t - \sigma)]^T \\ &= [x_1(t - \sigma), x_2(t - \sigma), x_5(t - \sigma), x_6(t - \sigma)]^T. \end{aligned} \quad (4)$$

Together with the associated dynamic equations

$$\begin{aligned} x_{sf}(t) &= x_c(t) + l_f \phi(t), \\ x_{ur}(t) &= x_c(t) - l_r \phi(t) \end{aligned} \quad (5)$$

and the definitions (2)–(4), the system (1) thus is rewritten in the state-space representation as

$$\begin{aligned} \dot{x}(t) &= Ax(t) + Bu(t - \tau) + Dv(t), \\ y_m(t) &= C_1x(t - \sigma), \\ y_c(t) &= C_2x(t) + Eu(t - \tau), \\ x(t) &= \alpha(t), \quad t \in [-\sigma, 0], \\ u(t) &= 0, \quad t \in [-\tau, 0], \end{aligned} \quad (6)$$

with $x(t) \in \mathbb{R}^8$, $u(t) \in \mathbb{R}^2$, $y_m(t) \in \mathbb{R}^4$, and $y_c(t) \in \mathbb{R}^6$ as the state vector, control output, measurement vector, and controlled output, respectively, A, B, C_1, C_2, D , and E as the real constant matrices of appropriate dimensions, and $\alpha(t) \in \mathbf{C}([-\sigma, 0]; \mathbb{R}^8)$ as the initial state vector.

Consequently, the sampled-data system form of the system (6) can be got by applying the sampled-data controller where there is a zero-order holder

$$\begin{aligned} u(t) &= u[t_k], \quad t \in [t_k, t_{k+1}), \\ u[t_k] &= u(Kx(t_{k-h_2-d_2})), \quad k \in \mathbb{N}_0, \\ u[t_k] &= 0, \quad k < 0, \end{aligned} \quad (7)$$

with $\{t_k\}$ as the sampling times, $x(t_k)$ as the state on time of $t_k = kT$, and K as a constant data controller gain, denoting the actuator delay $\tau = h_1T + d_1T$ and the sensor delay $\sigma = h_2T + d_2T$ with $h_i \in \mathbb{N}$ and $0 \leq d_i < 1$ ($i = 1, 2$). Notice

that the delays are expressed in either integers or nonintegers. Then, the sampled-data system of (1) can be described by

$$\begin{aligned} \dot{x}(t) &= Ax(t) + Bu(t_{k-h_1-d_1}) + Dv(t), \\ y_m(t) &= C_1x(t_{k-h_2-d_2}), \\ y_c(t) &= C_2x(t) + Eu(t_{k-h_1-d_1}), \quad t \in [t_k, t_{k+1}), \\ u(t_{k-h_1-d_1}) &= u(Kx(t_{k-h-d})), \end{aligned} \quad (8)$$

where $h = h_1 + h_2$ and $d = d_1 + d_2$. Here, the triple (A, B, C_1) is assumed to be completely controllable and observable.

Further, the sampled-data system (8) will be converted to delta domain and without actuator delays. There are two situations that should be considered concerning the nonintegral part d of the time delay: $d \in [0, 1]$ and $d \in [1, 2]$. However, the derivation procedures of these two situations are similar. So, for the sake of simplicity, the derivation procedure of the former situation will be presented in what follows.

Introducing the delta operator as

$$\delta(\cdot)(t_{k-d_2}) \triangleq \begin{cases} \frac{(\cdot)(t_{k+1-d_2}) - (\cdot)(t_{k-d_2})}{T}, & T \neq 0 \\ \frac{d(\cdot)(t)}{dt}, & T = 0 \end{cases} \quad (9)$$

and letting $t = (k + 1 - d_2)T$ and $t_0 = (k - d_2)T$ discretize the sampled-data system (8) in the delta-domain form

$$\begin{aligned} \delta x(t_{k-d_2}) &= \bar{A}x(t_{k-d_2}) + B_1u[t_{k-h_1}] \\ &\quad + B_2u[t_{k-h_1-1}] + \bar{D}v(t_{k-d_2}), \\ x(t_{-d_2}) &= \alpha_0, \\ y_m(t_k) &= C_1x(t_{k-h_2-d_2}), \\ y_c(t_{k-d_2}) &= C_2x(t_{k-d_2}) + Eu[t_{k-h_1-1}]. \end{aligned} \quad (10)$$

Noting that the system (10) is the delta-domain sampled-data system with actuator delays, for the convenience of calculation, it will be transformed without actuator delays using the model transformation approach. From the first

difference equation in (10), it follows the analytical expression of state response

$$\begin{aligned} x(t_{k-d_2}) &= A_z^k x(t_{-d_2}) + \sum_{j=0}^{k-1} A_z^{k-1-j} \bar{B} u[t_j] \\ &+ \sum_{j=0}^{k-1} A_z^{k-1-j} D_z v(t_{j-d_2}) - \sum_{j=k-h_1}^{k-1} A_z^{k-1-j} \bar{B}_1 u[t_j] \\ &- \sum_{j=k-h_1-1}^{k-1} A_z^{k-1-j} \bar{B}_2 u[t_j], \end{aligned} \quad (11)$$

where

$$\begin{aligned} \bar{A} &= \frac{A_z - I}{T}, \quad B_1 = \frac{B_{z1}}{T}, \quad B_2 = \frac{B_{z2}}{T}, \\ \bar{D} &= \frac{D_z}{T}, \quad A_z = e^{AT}, \quad \bar{B} = \bar{B}_1 + \bar{B}_2, \\ \bar{B}_1 &= A_z^{-h_1} B_{z1}, \quad \bar{B}_2 = A_z^{-h_1-1} B_{z2} \\ B_{z1} &= \int_0^{(1-d)T} e^{As} ds B, \quad B_{z2} = \int_{(1-d)T}^T e^{As} ds B, \\ D_z &= \int_0^T e^{As} ds D. \end{aligned} \quad (12)$$

Consequently, define a new state vector as

$$\begin{aligned} z(t_{k-d_2}) &= x(t_{k-d_2}) + \sum_{i=k-h_1}^{k-1} A_z^{k-1-i} \bar{B}_1 u[t_i] \\ &+ \sum_{j=k-h_1-1}^{k-1} A_z^{k-1-j} \bar{B}_2 u[t_j]. \end{aligned} \quad (13)$$

Equation (10) yields the analytical expression of state response for the transformed system

$$\begin{aligned} z(t_{k-d_2}) &= A_z^k z(t_{-d_2}) + \sum_{m=0}^{k-1} A_z^{k-1-m} \bar{B} u[t_m] \\ &+ \sum_{l=0}^{k-1} A_z^{k-1-l} D_z v(t_{l-d_2}), \\ z(t_{-d_2}) &= \alpha_0, \end{aligned} \quad (14)$$

which produces its state equation in delta-domain form

$$\begin{aligned} \delta z(t_{k-d_2}) &= \bar{A} z(t_{k-d_2}) + \bar{B} u[t_k] + \bar{D} v(t_{k-d_2}), \\ z(t_{-d_2}) &= \alpha_0. \end{aligned} \quad (15)$$

Through the same way, defining the new measured and controlled outputs

$$\begin{aligned} \bar{y}_m(t_k) &= y_m(t_k) \\ &+ \bar{C}_1 \left[\sum_{l=k-h_2}^{k-1} A_z^{k-1-l} D_z v(t_{l-d_2}) + \sum_{i=k-h}^{k-1} A_z^{k-1-i} \bar{B}_1 u[t_i] \right. \\ &\left. + \sum_{j=k-h-1}^{k-1} A_z^{k-1-j} \bar{B}_2 u[t_j] \right], \\ \bar{y}_c(t_{k-d_2}) &= y_c(t_{k-d_2}) \\ &+ C_2 \left[\sum_{i=k-h_1}^{k-1} A_z^{k-1-i} \bar{B}_1 u[t_i] + \sum_{j=k-h_1-1}^{k-1} A_z^{k-1-j} \bar{B}_2 u[t_j] \right] \\ &- E u[t_{k-h_1-1}], \end{aligned} \quad (16)$$

with $\bar{C}_1 = C_1 A_z^{-h_2}$, the output equations of the transformed system are got as follows

$$\begin{aligned} \bar{y}_m(t_k) &= \bar{C}_1 z(t_{k-d_2}), \\ \bar{y}_c(t_{k-d_2}) &= C_2 z(t_{k-d_2}). \end{aligned} \quad (17)$$

Then, the state equation (15) and the output equation (17) consist the transformed equivalent sampled-data system in delta domain without actuator delays:

$$\begin{aligned} \delta z(t_{k-d_2}) &= \bar{A} z(t_{k-d_2}) + \bar{B} u[t_k] + \bar{D} v(t_{k-d_2}), \\ z(t_{-d_2}) &= \alpha_0, \\ \bar{y}_m(t_k) &= \bar{C}_1 z(t_{k-d_2}), \\ \bar{y}_c(t_{k-d_2}) &= C_2 z(t_{k-d_2}). \end{aligned} \quad (18)$$

Furthermore, the road excitation should be described by an exosystem in delta domain in order to employ the state-space representation designing the OVC.

2.2. Road Disturbance Modeling. According to ISO 2631 standards, the road displacement power spectral density (PSD) is usually approximately represented in the formulation of

$$S(\Omega) = C_s \Omega^{-2} = 4^k \times 10^{-7} \cdot \Omega^{-2}, \quad (19)$$

with Ω as the spatial frequency, C_s as the road roughness constant, and k as the sort of the road as shown in Table 1.

TABLE I: Road grades and PSDs.

Road grade	A	B	C	D	E
$C_s (\times 10^{-7} \text{ m}^3/\text{rad})$	1	4	16	64	245
Road sort k	0	1	2	3	4

Due to the low-pass-filter characteristic of vehicle tires and suspension, the road displacement $x_{ri}(t)$ ($i = f, r$) can be approximately simulated by a finite Fourier series sum

$$x_{ri}(t) = \sum_{j=1}^p \xi_j(t) \triangleq \sum_{j=1}^p \phi_j \sin(\omega_j t + \theta_j), \quad (20)$$

where $\phi_j = 2^k/10^3 j \sqrt{l/10\pi}$ are the amplitudes, $\omega_j = j\omega_0$ are the frequencies with the time frequency internal $\omega_0 = 2\pi v_0/l$, θ_j are the random phases which follow a uniform distribution in $[0, 2\pi)$, v_0 is a constant horizontal velocity, l is the given road segment length, and positive integer p limits the considered frequency band.

Letting the disturbance state vector

$$w(t) = [\xi_1(t), \xi_2(t), \dots, \xi_p(t), \dot{\xi}_1(t), \dot{\xi}_2(t), \dots, \dot{\xi}_p(t)]^T \in \mathbb{R}^p, \quad (21)$$

the road velocity $v(t) = [\dot{x}_{rf}(t), \dot{x}_{rr}(t)]^T$ then is described by the exosystem

$$\begin{aligned} \dot{w}(t) &= Gw(t), \\ v(t) &= Fw(t) \end{aligned} \quad (22)$$

with

$$\begin{aligned} G &= \begin{bmatrix} \mathbf{0} & \mathbf{I}_p \\ G_1 & \mathbf{0} \end{bmatrix} \in \mathbb{R}^{2p \times 2p}, \\ G_1 &= \text{diag}\{-\omega_1^2, -\omega_2^2, \dots, -\omega_p^2\} \in \mathbb{R}^{p \times p}, \\ F &= \begin{bmatrix} \mathbf{0}_p & 1 & \dots & 1 \\ \mathbf{0}_p & 1 & \dots & 1 \end{bmatrix} \in \mathbb{R}^{2 \times 2p}, \end{aligned} \quad (23)$$

in which $\mathbf{0}$ and \mathbf{I}_p represent the zero matrix and the p -order identity matrix, respectively. Using delta operator (9), exosystem (22) is transformed into the delta-domain form

$$\begin{aligned} \delta w(t_{k-d_2}) &= \bar{G}w(t_{k-d_2}), \\ v(t_{k-d_2}) &= Fw(t_{k-d_2}), \\ v(t_k) &= 0, \quad k < 0, \end{aligned} \quad (24)$$

where $\bar{G} = (e^{GT} - I)/T$.

Hence, both the original system and the exosystem are transformed into the delta-domain sampled-data systems so that we would design the OVC for them.

2.3. Problem Formulation. The principal variables for the evaluation of the suspension system are sprung mass acceleration \ddot{x}_c and $\ddot{\phi}$ determining the ride comfort, suspension deflection $x_{si} - x_{ui}$ indicating the limit of vehicle body motion, and tire deflection $x_{ui} - x_{ri}$ ensuring the road holding ability. The purpose is to reduce the acceleration of vehicle body and decrease the dynamic tire forces for improving the road holding ability and the stability of vehicles facing road excitation.

In practice, control u and controlled output y_c are unable synchronously zero so that the general infinite-horizon performance index is not convergent. In this case, an average infinite-horizon performance index could be chosen as

$$J(\cdot) = \lim_{N \rightarrow \infty} \frac{1}{N} \sum_{k=0}^N [z^T(t_{k-d_2}) Q z(t_{k-d_2}) + u^T[t_k] R u[t_k]] \quad (25)$$

with $Q = C_2^T Q_0 C_2$, $Q_0 = \text{diag}\{q_i\}$ ($i = 1, 2, \dots, 6$) as positive semidefinite matrices and $R = \text{diag}\{r_j\}$ ($j = 1, 2$) as a positive definite matrix, assuming that $C^T C = Q$ with C an arbitrary matrix and the triple (\bar{A}, \bar{B}, C) completely controllable and observable.

Remark 1. When $d \in [1, 2]$, the delta-domain sampled-data system is described by

$$\begin{aligned} \delta x(t_{k-d_2}) &= \bar{A}x(t_{k-d_2}) + B_1 u[t_{k-h_1-1}] \\ &\quad + B_2 u[t_{k-h_1-2}] + \bar{D}v(t_{k-d_2}), \\ x(t_{-d_2}) &= \alpha_0, \\ y_m(t_k) &= C_1 x(t_{k-h_2-d_2}), \\ y_c(t_{k-d_2}) &= C_2 x(t_{k-d_2}) + E u[t_{k-h_1-2}], \end{aligned} \quad (26)$$

with

$$B_1 = \frac{1}{T} \int_0^{(d-1)T} e^{As} ds B, \quad B_2 = \frac{1}{T} \int_{(d-1)T}^T e^{As} ds B. \quad (27)$$

The derivation procedure of this situation is similar to that of $d \in [0, 1]$. It is omitted for the simplification reason.

3. Optimal Vibration Controller Design

3.1. Sampled-Data OVC Design

Theorem 2. Consider the optimal vibration control problem described by the time-delay sampled-data system (10) under disturbance (24) respecting the average performance index

(25). The optimal vibration control law is existent and unique and given by

$$u^* [t_k] = -R^{-1}\bar{B}^T \left(T\bar{A}^T + I \right)^{-1} \times \left\{ (P - TQ) \left[x(t_{k-d_2}) + \sum_{i=k-h_1}^{k-1} A_z^{k-1-i} \bar{B}_1 u [t_i] + \sum_{j=k-h_1-1}^{k-1} A_z^{k-1-j} \bar{B}_2 u [t_j] \right] + P_1 w(t_{k-d_2}) \right\}, \quad (28)$$

where P is the unique positive definite solution of Riccati equation:

$$\left(T\bar{A}^T + I \right) P \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \left(T\bar{A} + I \right) + TQ = P, \quad (29)$$

P_1 is the unique solution of Stein equation:

$$\begin{aligned} & \left(T\bar{A}^T + I \right) T \left[I - TP \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \bar{B}R^{-1}\bar{B}^T \right] P_1 \bar{G} - P_1 \\ & = -T \left(T\bar{A}^T + I \right) P \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \bar{D}F. \end{aligned} \quad (30)$$

Proof. According to Pontryagin's minimum principle, the optimal control problem combined by the system (18) and the performance index (25) results in the two-point boundary value problem in delta-operator form:

$$\begin{aligned} \begin{bmatrix} \delta z(t_{k-d_2}) \\ \delta \lambda(t_{k-d_2}) \end{bmatrix} &= \begin{bmatrix} \bar{A} & -\bar{B}R^{-1}\bar{B}^T \\ -Q & -\bar{A}^T \end{bmatrix} \begin{bmatrix} z(t_{k-d_2}) \\ \lambda(t_{k+1-d_2}) \end{bmatrix} \\ &+ \begin{bmatrix} \bar{D} \\ 0 \end{bmatrix} v(t_{k-d_2}), \\ \begin{bmatrix} z(t_{-d_2}) \\ \lambda(t_{\infty}) \end{bmatrix} &= \begin{bmatrix} \alpha_0 \\ 0 \end{bmatrix}, \end{aligned} \quad (31)$$

which yields

$$\begin{aligned} z(t_{k+1-d_2}) &= \left(T\bar{A} + I \right) z(t_{k-d_2}) \\ &- T\bar{B}R^{-1}\bar{B}^T \lambda(t_{k+1-d_2}) + \bar{D}v(t_{k-d_2}), \end{aligned} \quad (32a)$$

$$\lambda(t_{k-d_2}) = TQz(t_{k-d_2}) + \left(T\bar{A}^T + I \right) \lambda(t_{k+1-d_2}), \quad (32b)$$

with the optimal control law

$$u^* [t_k] = -R^{-1}\bar{B}^T \lambda(t_{k+1-d_2}). \quad (33)$$

From (31) or (32a) and (32b) it is clear that λ and z are the linear relationship, so denote the costate vector

$$\lambda(t_{k-d_2}) = Pz(t_{k-d_2}) + P_1 w(t_{k-d_2}). \quad (34)$$

Consequently, on one hand, together with (34) and (32a), it gives

$$\begin{aligned} z(t_{k+1-d_2}) &= \left(I + \bar{B}R^{-1}\bar{B}^T P \right)^{-1} \\ &\times \left[\left(T\bar{A} + I \right) z(t_{k-d_2}) \right. \\ &\left. + \left(\bar{D}F - \bar{B}R^{-1}\bar{B}^T P_1 \bar{G} \right) w(t_{k-d_2}) \right]. \end{aligned} \quad (35)$$

On the other hand, from (34) and (32b), the following equation holds:

$$\begin{aligned} (P - TQ) z(t_{k-d_2}) &= \left(T\bar{A}^T + I \right) Pz(t_{k+1-d_2}) \\ &+ \left[\left(T\bar{A}^T + I \right) P_1 \bar{G} - P_1 \right] w(t_{k-d_2}). \end{aligned} \quad (36)$$

Substituting (35) into (36) yields

$$\begin{aligned} & \left[\left(T\bar{A}^T + I \right) P \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \right. \\ & \times \left(T\bar{A} + I \right) + TQ - P \left. \right] z(t_{k-d_2}) \\ & + \left[\left(T\bar{A}^T + I \right) P_1 \bar{G} - P_1 \right. \\ & \left. - \left(T\bar{A}^T + I \right) P \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \right. \\ & \left. \times T \left(\bar{B}R^{-1}\bar{B}^T P_1 \bar{G} - \bar{D}F \right) \right] w(t_{k-d_2}) = 0. \end{aligned} \quad (37)$$

Due to $z(t_{k-d_2})$ and $w(t_{k-d_2})$ arbitrarily satisfying (37), it results in Riccati equation (29) and Stein equation (30).

Further, the uniqueness is to be proved. According to linear optimal regulator theory, there exists a unique positive definite solution P for Riccati equation (26) and the closed-loop system of (18) is asymptotically stable, which implies that matrix

$$\left(T\bar{A} + I \right)^T T \left[I - TP \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \bar{B}R^{-1}\bar{B}^T \right] \quad (38)$$

is Hurwitz, that is,

$$\begin{aligned} & \left| T\mu_i \left(\left(T\bar{A} + I \right)^T T \left[I - TP \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \bar{B}R^{-1}\bar{B}^T \right] + I \right) \right| \\ & < 1 \end{aligned} \quad (39)$$

for $i = 1, 2, \dots, n$. Moreover, since road disturbances are persistent and not asymptotically stable, this means that

$$\left| T\mu_j(\bar{G}) + 1 \right| = 1 \quad (40)$$

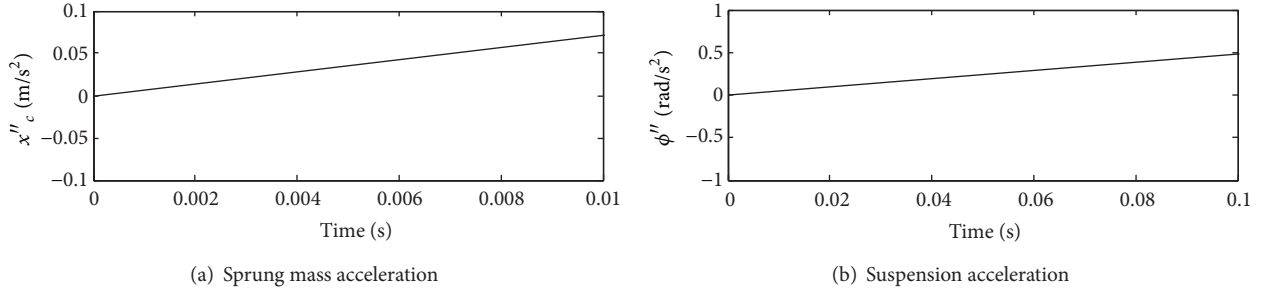


FIGURE 2: Acceleration responses of OLS.

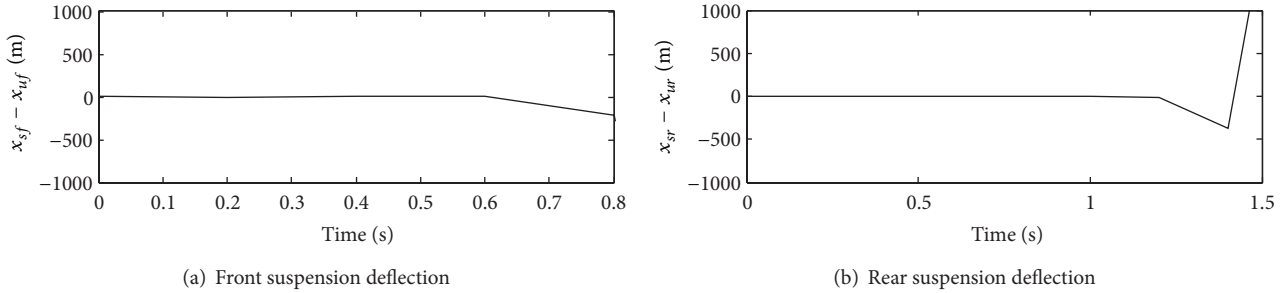


FIGURE 3: Suspension deflection responses of OLS.

for $j = 1, 2, \dots, p$. Therefore, from (39) and (40), the following inequality holds:

$$\left[\left| T\mu_i \left((T\bar{A} + I)^T T \right. \right. \right. \\ \left. \left. \times \left[I - TP \left(I + T\bar{B}R^{-1}\bar{B}^T P \right)^{-1} \bar{B}R^{-1}\bar{B}^T \right] \right) + 1 \right| \\ \left. \cdot \left| T\mu_j (\bar{G}) + 1 \right| \right] < 1. \quad (41)$$

As a result, Stein equation (30) has the unique solution matrix P_1 [16]. The uniqueness of P and P_1 leads to the uniqueness of OVC (28). This ends the proof. \square

3.2. *Physical Realization of OVC.* The optimal control law $u^*[t_k]$ (28) contains the physically unrealizable disturbance state $w(t_{k-d_2})$ and some unmeasurable variables in $x(t_{k-d_2})$ for economical or practical reasons. In this case, a reduced-order observer can be constructed to reconstruct these states. Defining the augmented vector $\zeta(t_{k-d_2}) = [z^T(t_{k-d_2}), w^T(t_{k-d_2})]^T$ and $\eta(t_{k-d_2}) = [\bar{y}_m^T(t_k), v^T(t_{k-d_2})]^T$ yields the following augmented system in delta domain combined by (18) and (24):

$$\begin{aligned} \delta\zeta(t_{k-d_2}) &= \bar{A}\zeta(t_{k-d_2}) + \bar{B}u[t_k], \\ \eta(t_{k-d_2}) &= \bar{C}\zeta(t_{k-d_2}), \end{aligned} \quad (42)$$

with

$$\bar{A} = \begin{bmatrix} \bar{A} & \bar{D}F \\ 0 & \bar{G} \end{bmatrix}, \quad \bar{B} = \begin{bmatrix} \bar{B} \\ 0 \end{bmatrix}, \quad \bar{C} = \begin{bmatrix} \bar{C}_1 & 0 \\ 0 & F \end{bmatrix}. \quad (43)$$

The pair (\bar{A}, \bar{C}) can be proved to be completely observable.

Choosing an arbitrary matrix H such that $\Gamma = [\bar{C}^T \ H^T]^T$ is nonsingular and defining $\Pi = \Gamma^{-1} = [\Pi_1 \ \Pi_2]$ give $\bar{C}\Gamma^{-1} = [I \ 0]$. Let the nonsingular transformation be as follows:

$$\bar{\zeta}(t_{k-d_2}) = \Gamma\zeta(t_{k-d_2}) \triangleq \begin{bmatrix} \bar{\zeta}_1(t_{k-d_2}) \\ \bar{\zeta}_2(t_{k-d_2}) \end{bmatrix}, \quad (44)$$

where $\eta(t_{k-d_2}) = \bar{\zeta}_1(t_{k-d_2})$. The new state equations follow in the delta-domain form:

$$\begin{aligned} \delta\bar{\zeta}_2(t_{k-d_2}) &= H\bar{A}\Pi_2\bar{\zeta}_2(t_{k-d_2}) + H\bar{A}\Pi_1\eta(t_{k-d_2}) + H\bar{B}u[t_k], \\ \delta\eta(t_{k-d_2}) &= \bar{C}\bar{A}\Pi_2\bar{\zeta}_2(t_{k-d_2}) + \bar{C}\bar{A}\Pi_1\eta(t_{k-d_2}) + \bar{C}\bar{B}u[t_k]. \end{aligned} \quad (45)$$

Defining a new variable

$$\psi(t_{k-d_2}) = \bar{\zeta}_2(t_{k-d_2}) - L\eta(t_{k-d_2}) \quad (46)$$

with L the gain matrix to be selected, (46) and (45) give

$$\begin{aligned} \delta\psi(t_{k-d_2}) &= (H - L\bar{C}) \left[\bar{A}\Pi_2\psi(t_{k-d_2}) + \bar{A}(\Pi_1 + \Pi_2L) \right. \\ &\quad \left. \times \eta(t_{k-d_2}) + \bar{B}u[t_k] \right], \\ \bar{\zeta}_2(t_{k-d_2}) &= \psi(t_{k-d_2}) + L\eta(t_{k-d_2}). \end{aligned} \quad (47)$$

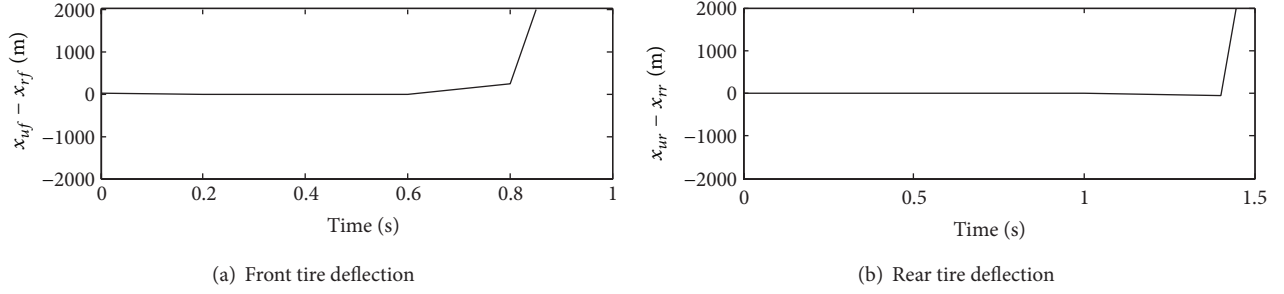
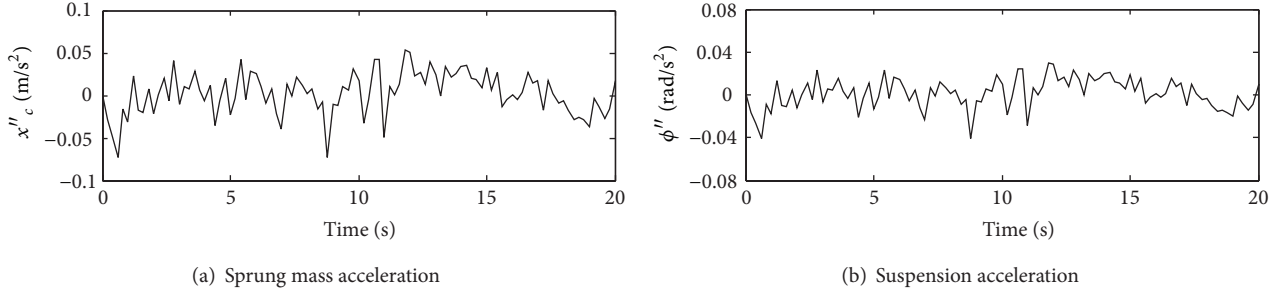


FIGURE 4: Tire deflection responses of OLS.

FIGURE 5: Acceleration responses under OVC with $\tau = 0.015$ s, $\sigma = 0.02$ s.

Noting that

$$\zeta(t_{k-d_2}) = \Pi_1 \eta(t_{k-d_2}) + \Pi_2 \bar{\zeta}_2(t_{k-d_2}) \quad (48)$$

and substituting (47) into (48) yield

$$\begin{aligned} \delta\psi(t_{k-d_2}) &= (H - L\bar{C}) \left[\bar{A}\Pi_2\psi(t_{k-d_2}) + \bar{A}(\Pi_1 + \Pi_2L) \right. \\ &\quad \left. \times \eta(t_{k-d_2}) + \bar{B}u[t_k] \right], \\ \zeta(t_{k-d_2}) &= \Pi_2\psi(t_{k-d_2}) + (\Pi_1 + \Pi_2L)\eta(t_{k-d_2}). \end{aligned} \quad (49)$$

Corresponding to (49), the reduced-order observer is constructed:

$$\begin{aligned} \delta\hat{\psi}(t_{k-d_2}) &= (H - L\bar{C}) \left[\bar{A}\Pi_2\hat{\psi}(t_{k-d_2}) + \bar{A}(\Pi_1 + \Pi_2L) \right. \\ &\quad \left. \times \eta(t_{k-d_2}) + \bar{B}u[t_k] \right], \\ \hat{\zeta}(t_{k-d_2}) &= \Pi_2\hat{\psi}(t_{k-d_2}) + (\Pi_1 + \Pi_2L)\eta(t_{k-d_2}), \end{aligned} \quad (50)$$

where $\hat{\psi}(t_{k-d_2})$ and $\hat{\zeta}(t_{k-d_2})$ are the state and output of the observer, respectively. Denoting observer errors $\tilde{\psi}(t_{k-d_2}) = \hat{\psi}(t_{k-d_2}) - \psi(t_{k-d_2})$ and $e(t_{k-d_2}) = \hat{\zeta}(t_{k-d_2}) - \zeta(t_{k-d_2})$, from (50) and (49), the error state equation is got:

$$\begin{aligned} \delta\tilde{\psi}(t_{k-d_2}) &= (H - L\bar{C}) \bar{A}\Pi_2\tilde{\psi}(t_{k-d_2}), \\ e(t_{k-d_2}) &= \Pi_2\tilde{\psi}(t_{k-d_2}). \end{aligned} \quad (51)$$

Hence, the error equation gain L should be regulated to make (51) asymptotically stable, such that $\lim_{k \rightarrow \infty} e(t_{k-d_2}) = 0$.

The observable pair (\bar{A}, \bar{C}) results in the observable pair $(\bar{C}\bar{A}\Pi_2, H\bar{A}\Pi_2)$. Consequentially, the gain L is enabled to make the eigenvalues of $(H - L\bar{C})\bar{A}\Pi_2$ assigned in the left-half complex plane, which means that error equation (51) is asymptotically stable. Therefore, the reconstructed states can replace the unavailable ones. Through this mean, states in OVC (28) are replaced by the augmented state

$$u[t_k] = -R^{-1}\bar{B}^T \left(T\bar{A}^T + I \right)^{-1} [P - TQ \ P_1] \hat{\zeta}(t_{k-d_2}), \quad (52)$$

which gives the dynamical control law

$$\begin{aligned} \delta\hat{\psi}(t_{k-d_2}) &= (H - L\bar{C}) \left[\bar{A}\Pi_2\hat{\psi}(t_{k-d_2}) + \bar{A}(\Pi_2L + \Pi_1) \right. \\ &\quad \left. \times \eta(t_{k-d_2}) + \bar{B}u[t_k] \right], \\ u[t_k] &= -R^{-1}\bar{B}^T \left(T\bar{A}^T + I \right)^{-1} [P - TQ \ P_1] \\ &\quad \times \left[\Pi_2\hat{\psi}(t_{k-d_2}) + (\Pi_1 + \Pi_2L)\eta(t_{k-d_2}) \right], \end{aligned} \quad (53)$$

with $\eta(t_{k-d_2}) = [\bar{y}_m^T(t_k), v^T(t_{k-d_2})]^T$ in which $\bar{y}_m(t_k)$ is defined in (16).

4. Simulation Examples

In this section, a half-car suspension model will be employed to carry out the simulations. We will take two cases of the simulations: firstly, to demonstrate the closed-loop matrices of the continues time, discrete time, and the delta domain taking different sampling period T in order to verify the delta-domain matrix enables approximating to the continues-time

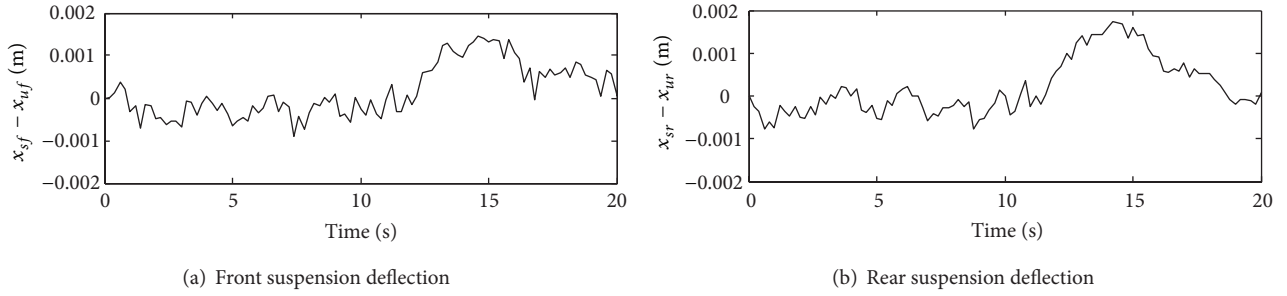


FIGURE 6: Suspension deflection responses under OVC with $\tau = 0.015$ s, $\sigma = 0.02$ s.

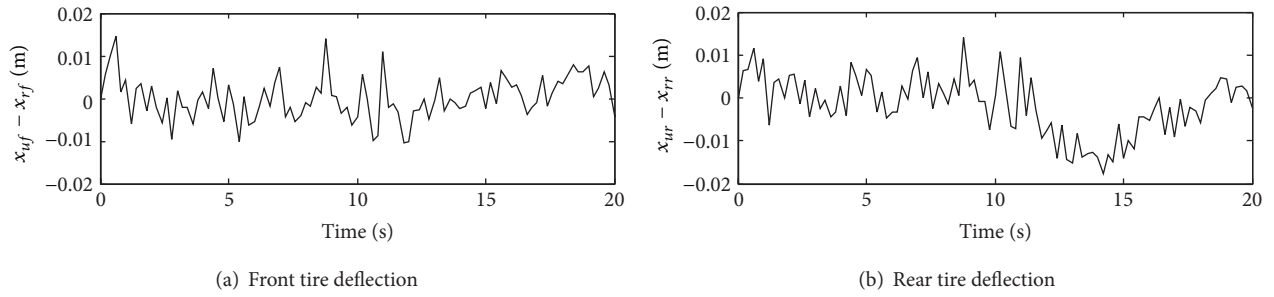


FIGURE 7: Tire deflection responses under OVC with $\tau = 0.015$ s, $\sigma = 0.02$ s.

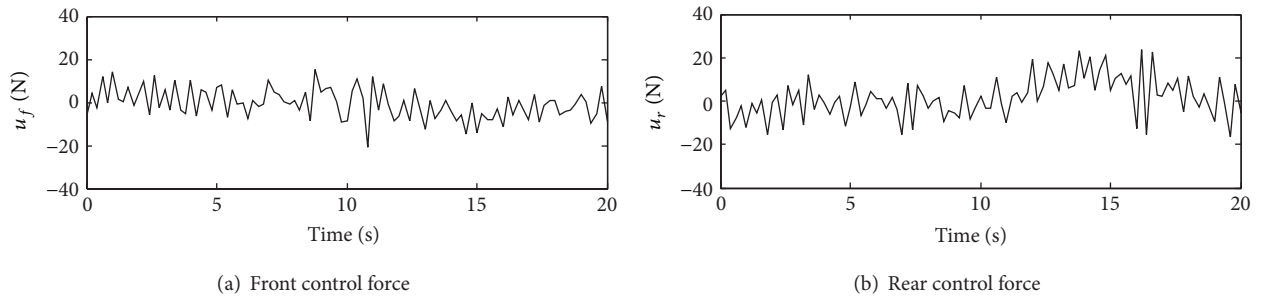


FIGURE 8: Control inputs of OVC with $\tau = 0.015$ s, $\sigma = 0.02$ s.

TABLE 2: Parameters of a half-car suspension.

Parameter	Variable	Value	Unit
Sprung mass	m_s	500	Kg
Sprung mass moment of inertia about pitch axis	I	910	$\text{Kg} \cdot \text{m}^2$
Front unsprung mass	m_{uf}	30	Kg
Rear unsprung mass	m_{ur}	40	Kg
Front suspension spring	k_f	10,000	N/m
Rear suspension spring	k_r	10,000	N/m
Front tire spring	k_{tf}	100,000	N/m
Rear tire spring	k_{tr}	100,000	N/m
Front suspension damper	b_f	1,000	$\text{N} \cdot \text{s/m}$
Rear suspension damper	b_r	1,000	$\text{N} \cdot \text{s/m}$
Distance from the center of mass to the front suspension attachment point	l_f	1.25	M
Distance from the center of mass to the rear suspension attachment point	l_r	1.45	M

one as T decreases; secondly, to apply the designed OVC to the half-car suspension model with delays comparing with the OLS in order to verify that the OVC guarantees the system stability and the desired suspension performance. The parameter values are shown in Table 2 (refer to in [15]).

To generate D Grade road profile, select $C_s = 64 \times 10^{-7} \text{ m}^3/\text{rad}$ and $k = 3$. Setting $v_0 = 20 \text{ m/s}$, $l = 400 \text{ m}$, and $p = 200$ in (20) takes the frequency band from 0.05 Hz to 20 Hz. Take the performance index (24) with $q_1 = q_2 = 10$,

$q_3 = q_4 = 10^3$, $q_5 = q_6 = 100$, $r_1 = r_2 = 10^{-3}$, and delays $\tau = 0.015 \text{ s}$, $\sigma = 0.02 \text{ s}$.

Case 1. Taking different sampling periods $T = 2 \text{ ms}$, 0.2 ms , 0.02 ms , the relative closed-loop matrices of continues-time A_c , discrete-time A_{cz} , and delta-domain $A_{c\delta}$ are listed from (54) to (56c); respectively.

(i) A_c is the continuous-time closed-loop matrix:

$$A_c = \begin{bmatrix} -7.2 & 135.7 & -18.4 & 260.9 & -0.8 & 380.6 & -5 & -0.5 \\ -17.6 & 113.6 & 118.1 & 221.3 & -3.2 & 368.7 & -1.1 & -1.8 \\ 4.5 & -16.7 & -39.8 & -32.9 & 0.7 & -62.1 & 0.8 & 0.2 \\ 17.4 & -111.9 & -116.7 & -218.1 & 3.1 & -362.3 & 1.1 & 1.7 \\ 141 & -2223.8 & -418.1 & -4215.2 & 34.5 & -7390.5 & 56 & 13.8 \\ -1.9 & 12.8 & 13.5 & 19 & -0.3 & 33 & 0 & -0.4 \\ 544.3 & -127.5 & -5667.5 & -295.7 & 63.7 & -1220.3 & -2.3 & 6.3 \\ 148.9 & -711.3 & -995.1 & -4372.8 & 26.7 & -3084.4 & 9.4 & -18.7 \end{bmatrix}. \quad (54)$$

(ii) A_{cz} is the discrete-time closed-loop matrix setting $T = 2 \text{ ms}$, 0.2 ms , 0.02 ms :

$T = 2 \text{ ms}$,

$$A_{cz} = \begin{bmatrix} 0.9826 & 0.2581 & 0.0035 & 0.4948 & -0.0019 & 0.7223 & -0.0098 & -0.0009 \\ -0.0342 & 1.2207 & 0.2305 & 0.4353 & -0.0061 & 0.7161 & -0.0020 & -0.0034 \\ 0.0094 & -0.0325 & 0.9160 & -0.0644 & 0.0015 & -0.1222 & 0.0015 & 0.0003 \\ 0.0337 & -0.2174 & -0.2277 & 0.5710 & 0.0061 & -0.7038 & 0.0020 & 0.0034 \\ 0.3096 & -4.3354 & -1.2278 & -8.2039 & 1.0709 & -14.4298 & 0.1099 & 0.0272 \\ -0.0037 & 0.0260 & 0.0266 & 0.0406 & -0.0006 & 1.0675 & -0.0001 & -0.0008 \\ 1.0441 & -0.2057 & -10.9210 & -0.5015 & 0.1222 & -2.2585 & 0.9883 & 0.0121 \\ 0.1870 & -0.7301 & -1.2585 & -7.2354 & 0.0336 & -3.8741 & 0.0112 & 0.9538 \end{bmatrix}, \quad (55a)$$

$T = 0.2 \text{ ms}$,

$$A_{cz} = \begin{bmatrix} 0.9985 & 0.0270 & -0.0033 & 0.0519 & -0.0002 & 0.0757 & -0.0010 & -0.0001 \\ -0.0035 & 1.0227 & 0.0236 & 0.0442 & -0.0006 & 0.0735 & -0.0002 & -0.0003 \\ 0.0009 & -0.0033 & 0.9920 & -0.0066 & 0.0001 & -0.0124 & 0.0002 & 0.0000 \\ 0.0035 & -0.0223 & -0.0233 & 0.9565 & 0.0006 & -0.0723 & 0.0002 & 0.0003 \\ 0.0285 & -0.4436 & -0.0877 & -0.8408 & 1.0069 & -1.4746 & 0.0112 & 0.0028 \\ -0.0004 & 0.0026 & 0.0027 & 0.0038 & -0.0001 & 1.0066 & 0.0000 & -0.0001 \\ 0.1084 & -0.0250 & -1.1295 & -0.0582 & 0.0127 & -0.2422 & 0.9995 & 0.0013 \\ 0.0286 & -0.1351 & -0.1915 & -0.8591 & 0.0051 & -0.5932 & 0.0018 & 0.9962 \end{bmatrix}, \quad (55b)$$

$T = 0.02 \text{ ms}$,

$$A_{cz} = \begin{bmatrix} 0.9999 & 0.0027 & -0.0004 & 0.0052 & 0.0000 & 0.0076 & -0.0001 & 0.0000 \\ -0.0004 & 1.0023 & 0.0024 & 0.0044 & -0.0001 & 0.0074 & 0.0000 & 0.0000 \\ 0.0001 & -0.0003 & 0.9992 & -0.0007 & 0.0000 & -0.0012 & 0.0000 & 0.0000 \\ 0.0003 & -0.0022 & -0.0023 & 0.9956 & 0.0001 & -0.0072 & 0.0000 & 0.0000 \\ 0.0028 & -0.0445 & -0.0084 & -0.0843 & 1.0007 & -0.1478 & 0.0011 & 0.0003 \\ 0.0000 & 0.0003 & 0.0003 & 0.0004 & 0.0000 & 1.0007 & 0.0000 & 0.0000 \\ 0.0109 & -0.0025 & -0.1133 & -0.0059 & 0.0013 & -0.0244 & 1.0000 & 0.0001 \\ 0.0030 & -0.0142 & -0.0198 & -0.0873 & 0.0005 & -0.0615 & 0.0002 & 0.9996 \end{bmatrix}. \quad (55c)$$

(iii) $A_{c\delta}$ is the delta-domain closed-loop matrix setting $T = 2 \text{ ms}, 0.2 \text{ ms}, 0.02 \text{ ms}$:

$$T = 2 \text{ ms},$$

$$A_{c\delta} = \begin{bmatrix} -8.7 & 129.1 & 1.7 & 247.4 & -0.9 & 361.2 & -4.9 & -0.5 \\ -17.1 & 110.4 & 115.2 & 217.7 & -3.1 & 358 & -1 & -1.7 \\ 4.7 & -16.2 & -42 & -32.2 & 0.8 & -61.1 & 0.8 & 0.2 \\ 16.9 & -108.7 & -113.8 & -214.5 & 3 & -351.9 & 1 & 1.7 \\ 154.8 & -2167.7 & -613.9 & -4101.9 & 35.4 & -7214.9 & 55 & 13.6 \\ -1.9 & 13 & 13.3 & 20.3 & -0.3 & 33.7 & 0 & -0.4 \\ 522 & -102.8 & -5460.5 & -250.7 & 61.1 & -1129.2 & -5.9 & 6 \\ 93.5 & -365.1 & -629.3 & -3617.7 & 16.8 & -1937.1 & 5.6 & -23.1 \end{bmatrix}, \tag{56a}$$

$$T = 0.2 \text{ ms},$$

$$A_{c\delta} = \begin{bmatrix} -7.4 & 135 & -16.3 & 259.5 & -0.8 & 378.6 & -0.5 & -0.5 \\ -17.6 & 113.3 & 117.9 & 221 & -3.2 & 367.6 & -1.1 & -1.7 \\ 4.6 & -16.6 & -40 & -32.9 & 0.7 & -62 & 0.8 & 0.2 \\ 17.4 & -111.6 & -116.5 & -217.7 & 3.1 & -361.3 & 1.1 & 1.7 \\ 142.5 & -2218.2 & -438.3 & -4203.8 & 34.6 & -7372.8 & 55.9 & 13.8 \\ -1.9 & 12.9 & 13.5 & 19.2 & -0.3 & 33.1 & 0 & -0.4 \\ 542.2 & -125 & -5647.6 & -291.1 & 63.4 & -1211.2 & -2.7 & 6.3 \\ 143.2 & -675.5 & -957.6 & -4295.4 & 25.7 & -2966.1 & 9 & -19.1 \end{bmatrix}, \tag{56b}$$

$$T = 0.02 \text{ ms},$$

$$A_{c\delta} = \begin{bmatrix} -7.2 & 135.6 & -18.2 & 260.8 & -0.8 & 380.4 & -5 & -0.5 \\ -17.6 & 113.6 & 118.1 & 221.3 & -3.2 & 368.6 & -1.1 & -1.8 \\ 4.5 & -16.7 & -39.8 & -32.9 & 0.7 & -62.1 & 0.8 & 0.2 \\ 17.4 & -111.9 & -116.7 & -218 & 3.1 & -362.2 & 1.1 & 1.7 \\ 141.2 & -2223.3 & -420.2 & -4214.1 & 34.6 & -7388.7 & 56 & 13.8 \\ -1.9 & 12.8 & 13.5 & 19 & -0.3 & 33 & 0 & -0.4 \\ 544.1 & -127.2 & -5665.5 & -295.2 & 63.7 & -1219.4 & -2.3 & 6.3 \\ 148.3 & -707.7 & -991.3 & -4365 & 26.6 & -3072.6 & 9.4 & -18.7 \end{bmatrix}. \tag{56c}$$

Comparing with the continuous-time closed-loop matrix (54), from (55a) to (55c) we can see the discretized matrices approach to the unit matrix as the sampling period T decreases; from (56a) to (56c) we can see that the delta-domain matrices approach to the original continuous-time matrix (54) as T decreases. Evidently, the delta-domain approach is more appropriate for the high-sampling IVNs system.

Case 2. Setting sampling period $T = 0.2 \text{ s}$ and comparing with the responses of the accelerations, deflections of suspension and tire, and control input of OLS shown in Figures 2, 3, and 4, the suspension responses controlled by OVC are shown in Figures 5, 6, 7, and 8.

System responses in Figures 2–4 show that they diverged when without control (of OLS). On the contrary, in Figures 5–8, when the suspension was controlled under OVC, the suspension responses were stabilized. Moreover, they achieved relatively low magnitude and satisfied the desired requirement.

5. Conclusions

This paper has presented the OVC design for sampled-data system with time delays with its application to a half-car suspension using delta-domain approach. Through this approach, the built model provides more realistic and appropriate property. The delay compensators guarantee the closed-loop stability and requested performance. The simulation has demonstrated that the designed controller can efficiently make the system performance achieve the desired goal and the design approach proposed in this study is effective and feasible.

Acknowledgments

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